DESCRIPTION
The NE/SE567 tone and frequency decoder is a highly stable phase-locked loop with synchronous AM lock detection and power output circuitry. Its primary function is to drive a load whenever a sustained frequency within its detection band is present at the self-biased input. The bandwidth center frequency and output delay are independently determined by means of four external components.

FEATURES
- Wide frequency range (.01Hz to 500kHz)
- High stability of center frequency
- Independently controllable bandwidth (up to 14%)
- High out-band signal and noise rejection
- Logic-compatible output with 100mA current sinking capability
- Inherent immunity to false signals
- Frequency adjustment over a 20-to-1 range with an external resistor
- Military processing available

APPLICATIONS
- Touch-Tone® decoding
- Carrier current remote controls
- Ultrasonic controls (remote TV, etc.)
- Communications paging

BLOCK DIAGRAM

@Touch-Tone is a registered trademark of AT&T.
## ORDERING INFORMATION

<table>
<thead>
<tr>
<th>DESCRIPTION</th>
<th>TEMPERATURE RANGE</th>
<th>ORDER CODE</th>
<th>DWG #</th>
</tr>
</thead>
<tbody>
<tr>
<td>8-Pin Plastic SO</td>
<td>0 to +70°C</td>
<td>NE567D</td>
<td>0174C</td>
</tr>
<tr>
<td>14-Pin Cerdip</td>
<td>0 to +70°C</td>
<td>NE567F</td>
<td>0581B</td>
</tr>
<tr>
<td>8-Pin Plastic DIP</td>
<td>0 to +70°C</td>
<td>NE567N</td>
<td>0404B</td>
</tr>
<tr>
<td>8-Pin Plastic SO</td>
<td>-55°C to +125°C</td>
<td>SE567D</td>
<td>0174C</td>
</tr>
<tr>
<td>8-Pin Cerdip</td>
<td>-55°C to +125°C</td>
<td>SE567FE</td>
<td>0581B</td>
</tr>
<tr>
<td>8-Pin Plastic DIP</td>
<td>-55°C to +125°C</td>
<td>SE567N</td>
<td>0404B</td>
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</table>

## ABSOLUTE MAXIMUM RATINGS

<table>
<thead>
<tr>
<th>SYMBOL</th>
<th>PARAMETER</th>
<th>RATING</th>
<th>UNIT</th>
</tr>
</thead>
<tbody>
<tr>
<td>T_A</td>
<td>Operating temperature</td>
<td>NE567 0 to +70</td>
<td>°C</td>
</tr>
<tr>
<td></td>
<td></td>
<td>SE567 -55 to +125</td>
<td>°C</td>
</tr>
<tr>
<td>V_CC</td>
<td>Operating voltage</td>
<td>10</td>
<td>V</td>
</tr>
<tr>
<td>V+_</td>
<td>Positive voltage at input</td>
<td>0.5 +V_S</td>
<td>V</td>
</tr>
<tr>
<td>V_-</td>
<td>Negative voltage at input</td>
<td>-10</td>
<td>VDC</td>
</tr>
<tr>
<td>V_OUT</td>
<td>Output voltage (collector of output transistor)</td>
<td>15</td>
<td>VDC</td>
</tr>
<tr>
<td>T_STG</td>
<td>Storage temperature range</td>
<td>-65 to +150</td>
<td>°C</td>
</tr>
<tr>
<td>P_D</td>
<td>Power dissipation</td>
<td>300</td>
<td>mW</td>
</tr>
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</table>
## DC ELECTRICAL CHARACTERISTICS

V +=5.0V; T A =25°C, unless otherwise specified.

<table>
<thead>
<tr>
<th>SYMBOL</th>
<th>PARAMETER</th>
<th>TEST CONDITIONS</th>
<th>SE567</th>
<th>NE567</th>
<th>UNIT</th>
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</thead>
<tbody>
<tr>
<td>fO</td>
<td>Highest center frequency</td>
<td>-55 to +125°C</td>
<td>500</td>
<td>500</td>
<td>kHz</td>
</tr>
<tr>
<td>fO</td>
<td>Center frequency stability</td>
<td>0 to +70°C</td>
<td>35 ±140</td>
<td>35 ±140</td>
<td>ppm/°C</td>
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<tr>
<td>fO</td>
<td>Center frequency distribution</td>
<td>-10</td>
<td>0</td>
<td>+10</td>
<td>-10</td>
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<tr>
<td>fO</td>
<td>Center frequency shift with supply voltage</td>
<td>0.5</td>
<td>1</td>
<td>0.7</td>
<td>2</td>
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Detection bandwidth

<table>
<thead>
<tr>
<th>BW</th>
<th>Largest detection bandwidth</th>
<th>fO = 100kHz = 1/1.1R1C1</th>
<th>12</th>
<th>14</th>
<th>16</th>
<th>10</th>
<th>14</th>
<th>18</th>
<th>% of fO</th>
</tr>
</thead>
</table>

Input

<table>
<thead>
<tr>
<th>RIN</th>
<th>Input resistance</th>
<th>15</th>
<th>20</th>
<th>25</th>
<th>15</th>
<th>20</th>
<th>25</th>
<th>kΩ</th>
</tr>
</thead>
<tbody>
<tr>
<td>V1</td>
<td>Smallest detectable input voltage</td>
<td>lI=100mA, fI=fO</td>
<td>20</td>
<td>25</td>
<td>20</td>
<td>25</td>
<td>mV RMS</td>
<td></td>
</tr>
<tr>
<td></td>
<td>Largest no-output input voltage</td>
<td>lI=100mA, fI=fO</td>
<td>10</td>
<td>15</td>
<td>10</td>
<td>15</td>
<td>mV RMS</td>
<td></td>
</tr>
<tr>
<td></td>
<td>Greatest simultaneous out-band signal-to-in-band signal ratio</td>
<td>+6</td>
<td>+6</td>
<td>dB</td>
<td></td>
<td></td>
<td></td>
<td></td>
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<tr>
<td></td>
<td>Minimum input signal to wide-band noise ratio</td>
<td>Bn=140kHz</td>
<td>-6</td>
<td>-6</td>
<td>dB</td>
<td></td>
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Output

<table>
<thead>
<tr>
<th>fO/20</th>
<th>Fastest on-off cycling rate</th>
<th>Vb=15V</th>
<th>0.01</th>
<th>25</th>
<th>0.01</th>
<th>25</th>
<th>μA</th>
</tr>
</thead>
<tbody>
<tr>
<td>fO/20</td>
<td>“1” output leakage current</td>
<td>Vb=15V</td>
<td>0.2</td>
<td>0.4</td>
<td>0.2</td>
<td>0.4</td>
<td>V</td>
</tr>
<tr>
<td></td>
<td>“0” output voltage</td>
<td>lI=30mA</td>
<td>0.6</td>
<td>1.0</td>
<td>0.6</td>
<td>1.0</td>
<td>V</td>
</tr>
<tr>
<td></td>
<td>lI=100mA</td>
<td>0.6</td>
<td>1.0</td>
<td>0.6</td>
<td>1.0</td>
<td>V</td>
<td></td>
</tr>
<tr>
<td>tF</td>
<td>Output fall time</td>
<td>R_L=50Ω</td>
<td>30</td>
<td>30</td>
<td>ns</td>
<td></td>
<td></td>
</tr>
<tr>
<td>tR</td>
<td>Output rise time</td>
<td>R_L=50Ω</td>
<td>150</td>
<td>150</td>
<td>ns</td>
<td></td>
<td></td>
</tr>
</tbody>
</table>

General

<table>
<thead>
<tr>
<th>VCC</th>
<th>Operating voltage range</th>
<th>4.75</th>
<th>9.0</th>
<th>4.75</th>
<th>9.0</th>
<th>V</th>
</tr>
</thead>
<tbody>
<tr>
<td></td>
<td>Supply current quiescent</td>
<td>6</td>
<td>8</td>
<td>7</td>
<td>10</td>
<td>mA</td>
</tr>
<tr>
<td></td>
<td>Supply current—activated</td>
<td>R_L=20kΩ</td>
<td>11</td>
<td>13</td>
<td>12</td>
<td>15</td>
</tr>
<tr>
<td>tPD</td>
<td>Quiescent power dissipation</td>
<td>30</td>
<td>35</td>
<td>mW</td>
<td></td>
<td></td>
</tr>
</tbody>
</table>

NOTES:
1. Frequency determining resistor R1 should be between 2 and 20kΩ.
2. Applicable over 4.75V to 5.75V. See graphs for more detailed information.
3. Pin 8 to Pin 1 feedback R_L network selected to eliminate pulsing during turn-on and turn-off.
4. With R2=130kΩ from Pin 1 to V+. See Figure 1.
TYPICAL PERFORMANCE CHARACTERISTICS

Bandwidth vs Input Signal Amplitude

Largest Detection bandwidth vs Operating Frequency

Detection bandwidth as a Function of $C_2$ and $C_3$

Typical Supply Current vs Supply Voltage

Greatest Number of Cycles Before Output

Typical Output Voltage vs Temperature

Typical Frequency Drift With Temperature (Mean and SD)

Typical Frequency Drift With Temperature (Mean and SD)

Typical Frequency Drift With Temperature (Mean and SD)
TYPICAL PERFORMANCE CHARACTERISTICS (Continued)

<table>
<thead>
<tr>
<th>Center Frequency Temperature Coefficient (Mean and SD)</th>
<th>Center Frequency Shift With Supply Voltage Change vs Operating Frequency</th>
<th>Typical Bandwidth Variation Temperature</th>
</tr>
</thead>
</table>

- **Center Frequency Temperature Coefficient**
  - **Temperature**: -300°C to 70°C
  - **Supply Voltage**: 4.5 V to 7.0 V

- **Center Frequency Shift**
  - With Supply Voltage Change

- **Operating Frequency**
  - **Typical Bandwidth Variation**
    - **Temperature**: -75°C to 125°C

DESIGN FORMULAS

\[
\frac{f_0}{1.1R_1C_1} = \frac{V_i}{f_0C_2} \quad \text{in } \% \text{ of } f_0
\]

Where

- \(V_i\) = Input voltage (V RMS)
- \(C_2\) = Low-pass filter capacitor (µF)

PHASE-LOCKED LOOP TERMINOLOGY CENTER FREQUENCY \(f_0\)

The free-running frequency of the current controlled oscillator (CCO) in the absence of an input signal.

Detection Bandwidth (BW)

The frequency range, centered about \(f_0\), within which an input signal above the threshold voltage (typically 20mV RMS) will cause a logical zero state on the output. The detection bandwidth corresponds to the loop capture range.

Lock Range

The largest frequency range within which an input signal above the threshold voltage will hold a logical zero state on the output.

Detection Band Skew

A measure of how well the detection band is centered about the center frequency, \(f_0\). The skew is defined as \(\frac{(f_{\text{MAX}} - f_{\text{MIN}})}{2f_0}\), where \(f_{\text{MAX}}\) and \(f_{\text{MIN}}\) are the frequencies corresponding to the edges of the detection band. The skew can be reduced to zero if necessary by means of an optional centering adjustment.

OPERATING INSTRUCTIONS

Figure 1 shows a typical connection diagram for the 567. For most applications, the following three-step procedure will be sufficient for choosing the external components \(R_1, C_1, C_2,\) and \(C_3\).

1. Select \(R_1\) and \(C_1\) for the desired center frequency. For best temperature stability, \(R_1\) should be between 2K and 20K ohm, and the combined temperature coefficient of the \(R_1C_1\) product should have sufficient stability over the projected temperature range to meet the necessary requirements.

2. Select the low-pass capacitor, \(C_2\), by referring to the Bandwidth versus Input Signal Amplitude graph. If the input amplitude variation is known, the appropriate value of \(f_0\cdot C_2\) necessary to give the desired bandwidth may be found. Conversely, an area of operation may be selected on this graph and the input level and \(C_2\) may be adjusted accordingly. For example, constant bandwidth operation requires that input amplitude be above 200mV RMS. The bandwidth, as noted on the graph, is then controlled solely by the \(f_0\cdot C_2\) product (\(f_0\) (Hz), \(C_2\) (µF)).
TYPICAL RESPONSE

Response to 100mV RMS Tone Burst

NOTES:
R₁ = 100Ω
S/N = –6dB
Noise Bandwidth = 140Hz

Response to Same Input Tone Burst With Wideband Noise

3. The value of C₃ is generally non-critical. C₃ sets the band edge of a low-pass filter which attenuates frequencies outside the detection band to eliminate spurious outputs. If C₃ is too small, frequencies just outside the detection band will switch the output stage on and off at the beat frequency, or the output may pulse on and off during the turn-on transient. If C₃ is too large, turn-on and turn-off of the output stage will be delayed until the voltage on C₃ passes the threshold voltage. (Such delay may be desirable to avoid spurious outputs due to transient frequencies.) A typical minimum value for C₃ is 2C₂.

4. Optional resistor R₂ sets the threshold for the largest “no output” input voltage. A value of 130kΩ is used to assure the tested limit of 10mVRMS min. This resistor can be referenced to ground for increased sensitivity. The explanation can be found in the “optional controls” section which follows.

AVAILABLE OUTPUTS (Figure 1)
The primary output is the uncommitted output transistor collector, Pin 8. When an in-band input signal is present, the transistor saturates; its collector voltage being less than 1.0 volt (typically 0.6V) at full output current (100mA). The voltage at Pin 2 is the phase detector output which is a linear function of frequency over the range of 0.95 to 1.05f₀ with a slope of about 20mV per percent of frequency deviation. The average voltage at Pin 1 is, during lock, a function of the in-band input amplitude in accordance with the transfer characteristic given. Pin 5 is the controlled oscillator square wave output of magnitude (+V –2VBE)=(+V-1.4V) having a DC average of +V/2. A 1kΩ load may be driven from pin 5. Pin 6 is an exponential triangle of 1VP-P with an average DC level of +V/2. Only high impedance loads may be

Figure 2. Typical Output Response
Tone decoder/phase-locked loop

OPERATING PRECAUTIONS
A brief review of the following precautions will help the user achieve the high level of performance of which the 567 is capable.

1. Operation in the high input level mode (above 200mV) will free the user from bandwidth variations due to changes in the in-band signal amplitude. The input stage is now limiting, however, so that out-band signals or high noise levels can cause an apparent bandwidth reduction as the inband signal is suppressed. Also, the limiting action will create in-band components from sub-harmonic signals, so the 567 becomes sensitive to signals at fO/3, fO/5, etc.

2. The 567 will lock onto signals near (2n+1) fO, and will give an output for signals near (4n+1) fO where n=0, 1, 2, etc. Thus, signals at 5fO and 9fO can cause an unwanted output. If such signals are anticipated, they should be attenuated before reaching the 567 input.

3. Maximum immunity from noise and out-band signals is afforded in the low input level (below 200mVRMS) and reduced bandwidth operating mode. However, decreased loop damping causes the worst-case lock-up time to increase, as shown by the Greatest Number of Cycles Before Output vs Bandwidth graph.

4. Due to the high switching speeds (20ns) associated with 567 operation, care should be taken in lead routing. Lead lengths should be kept to a minimum. The power supply should be adequately bypassed close to the 567 with a 0.01µF or greater capacitor; grounding paths should be carefully chosen to avoid ground loops and unwanted voltage variations. Another factor which must be considered is the effect of load energization on the power supply. For example, an incandescent lamp typically draws 10 times rated current at turn-on. This can be somewhat greater when the output stage is made less sensitive, rejection of the third harmonics or in-band harmonics (of lower frequency signals) is also improved.

SPEED OF OPERATION
Minimum lock-up time is related to the natural frequency of the loop. The lower it is, the longer becomes the turn-on transient. Thus, maximum operating speed is obtained when C2 is at a minimum. When the signal is first applied, the phase may be such as to initially drive the controlled oscillator away from the incoming frequency rather than toward it. Under this condition, which is of course unpredictable, the lock-up transient is at its worst and the theoretical minimum lock-up time is not achievable. We must simply wait for the transient to die out.

The following expressions give the values of C2 and C3 which allow highest operating speeds for various band center frequencies. The minimum rate at which digital information may be detected without information loss due to the turn-on transient or output chatter is about 10 cycles per bit, corresponding to an information transfer rate of fO/10 baud.
In cases where turn-off time can be sacrificed to achieve fast turn-on, the optional sensitivity adjustment circuit can be used to move the quiescent \( C_3 \) voltage lower (closer to the threshold voltage). However, sensitivity to beat frequencies, noise and extraneous signals will be increased.

**OPTIONAL CONTROLS** (Figure 3)
The 567 has been designed so that, for most applications, no external adjustments are required. Certain applications, however, will be greatly facilitated if full advantage is taken of the added control possibilities available through the use of additional external components. In the diagrams given, typical values are suggested where applicable. For best results the resistors used, except where noted, should have the same temperature coefficient. Ideally, silicon diodes would be low-resistivity types, such as forward-biased transistor base-emitter junctions. However, ordinary low-voltage diodes should be adequate for most applications.

**SENSITIVITY ADJUSTMENT** (Figure 3)
When operated as a very narrow-band detector (less than 8 percent), both \( C_2 \) and \( C_3 \) are made quite large in order to improve noise and out-band signal rejection. This will inevitably slow the response time. If, however, the output stage is biased closer to the threshold level, the turn-on time can be improved. This is accomplished by drawing additional current to terminal 1. Under this condition, the 567 will also give an output for lower-level signals (10mV or lower).

By adding current to terminal 1, the output stage is biased further away from the threshold voltage. This is most useful when, to obtain maximum operating speed, \( C_2 \) and \( C_3 \) are made very small. Normally, frequencies just outside the detection band could cause false outputs under this condition. By desensitizing the output stage, the out-band beat notes do not feed through to the output stage. Since the input level must

---

\[
C_2 = \frac{130}{f_{O}} \ F
\]

\[
C_3 = \frac{260}{f_{O}} \ F
\]
CHATTER PREVENTION  (Figure 4)
Chatter occurs in the output stage when $C_3$ is relatively small, so that the lock transient and the AC components at the quadrature phase detector (lock detector) output cause the output stage to move through its threshold more than once. Many loads, for example lamps and relays, will not respond to the chatter. However, logic may recognize the chatter as a series of outputs. By feeding the output stage output back to its input (Pin 1) the chatter can be eliminated. Three schemes for doing this are given in Figure 4. All operate by feeding the first output step (either on or off) back to the input, pushing the input past the threshold until the transient conditions are over. It is only necessary to assure that the feedback time constant is not so large as to prevent operation at the highest anticipated speed. Although chatter can always be eliminated by making $C_3$ large, the feedback circuit will enable faster operation of the 567 by allowing $C_3$ to be kept small. Note that if the feedback time constant is made quite large, a short burst at the input frequency can be stretched into a long output pulse. This may be useful to drive, for example, stepping relays.

DETECTION BAND CENTERING (OR SKEW) ADJUSTMENT  (Figure 5)
When it is desired to alter the location of the detection band (corresponding to the loop capture range) within the lock range, the circuits shown above can be used. By moving the detection band to one edge of the range, for example, input signal variations will expand the detection band in only one direction. This may prove useful when a strong but undesirable signal is expected on one side or the other of the center frequency. Since $R_B$ also alters the duty cycle slightly, this method may be used to obtain a precise duty cycle when the 567 is used as an oscillator.

ALTERNATE METHOD OF BANDWIDTH REDUCTION (Figure 6)
Although a large value of $C_2$ will reduce the bandwidth, it also reduces the loop damping so as to slow the circuit response time. This may be undesirable. Bandwidth can be reduced by reducing the loop gain. This scheme will improve damping and permit faster operation under narrow-band conditions. Note that the reduced impedance level at terminal 2 will require that a larger value of $C_2$ be used for a given filter cutoff frequency. If more than three 567s are to be used, the network of $R_B$ and $R_C$ can be eliminated and the $R_A$ resistors connected together. A capacitor between this junction and ground may be required to shunt high frequency components.

OUTPUT LATCHING  (Figure 7)
To latch the output on after a signal is received, it is necessary to provide a feedback resistor around the output stage (between Pins 8 and 1). Pin 1 is pulled up to unlatch the output stage.

REDUCTION OF C1 VALUE
For precision very low-frequency applications, where the value of $C_1$ becomes large, an overall cost savings may be achieved by inserting a voltage-follower between the $R_1$ $C_1$ junction and Pin 6, so as to allow a higher value of $R_1$ and a lower value of $C_1$ for a given frequency.

PROGRAMMING
To change the center frequency, the value of $R_1$ can be changed with a mechanical or solid state switch, or additional $C_1$ capacitors may be added by grounding them through saturating NPN transistors.
TYPICAL APPLICATIONS

NOTES:
Component values (Typical)
- $R_1 = 26.8 \text{ to } 15\, \text{k}\Omega$
- $R_2 = 24.7\, \text{k}\Omega$
- $R_3 = 20\, \text{k}\Omega$
- $C_1 = 0.10\, \text{mF}$
- $C_2 = 1.0\, \text{mF} \ 5\, \text{V}$
- $C_3 = 2.2\, \text{mF} \ 6\, \text{V}$
- $C_4 = 250\, \mu\text{F} \ 6\, \text{V}$
TYPICAL APPLICATIONS (Continued)

1. Resistor and capacitor values chosen for desired frequencies and bandwidth.
2. If C3 is made large so as to delay turn-on of the top 567, decoding of sequential \( f_1, f_2 \) tones is possible.
TYPICAL APPLICATIONS (Continued)

- Oscillator With Quadrature Output
- Oscillator With Double Frequency Output
- Precision Oscillator With 20ns Switching
- Pulse Generator With 25% Duty Cycle
- Precision Oscillator to Switch 100mA Loads
- Pulse Generator